



# 18-BIT, 1-MSPS, PSEUDO-DIFFERENTIAL UNIPOLAR INPUT, MICROWATT SAMPLING ANALOG-TO-DIGITAL CONVERTER WITH PARALLEL INTERFACE AND REFERENCE

## FEATURES

- 0 to 1 MSPS Sampling Rate
- 18-Bit NMC Ensured Over Temperature
- Low  $\pm 0.1$  mV Offset Error
- Low 0.2 ppm/ $^{\circ}$ C Offset Error Temperature Drift
- Low 0.6 ppm/ $^{\circ}$ C Gain Error Temperature Drift
- Zero Latency
- Low Power: 220 mW at 1 MSPS
- Unipolar Single-Ended Input Range: 0 V to  $V_{ref}$
- Onboard Reference
- Onboard Reference Buffer
- High-Speed Parallel Interface
- Wide Digital Supply 2.7 V ~ 5.25 V
- 8-/16-/18-Bit Bus Transfer
- 7x7 QFN Package

## APPLICATIONS

- Medical Instruments
- Optical Networking
- Transducer Interface
- High Accuracy Data Acquisition Systems
- Magnetometers

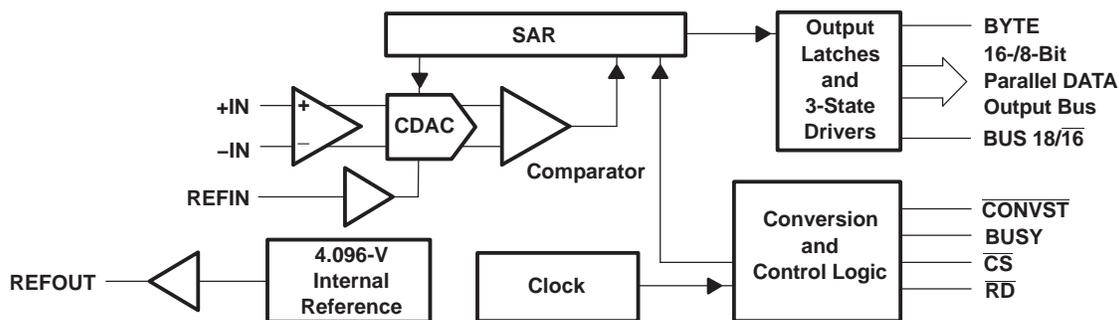
## DESCRIPTION

The ADS8481 is an 18-bit, 1-MSPS A/D converter with an internal 4.096-V reference and a pseudo-differential unipolar single-ended input. The device includes a 18-bit capacitor-based SAR A/D converter with inherent sample and hold. The ADS8481 offers a full 18-bit interface, a 16-bit option where data is read using two read cycles, or an 8-bit bus option using three read cycles.

The ADS8481 is available in a 7x7 QFN package and is characterized over the industrial  $-40^{\circ}$ C to  $85^{\circ}$ C temperature range.

## HIGH SPEED SAR CONVERTER FAMILY

TYPE/SPEED	500 kHz	580 kHz	750 kHz	1 MHz	1.25 MHz	2 MHz	3 MHz	4MHz
18-Bit Pseudo-Diff	ADS8383	ADS8381		ADS8481				
		ADS8380(S)						
18-Bit Pseudo-Bipolar, Fully Diff		ADS8382(S)		ADS8482				
16-Bit Pseudo-Diff			ADS8371	ADS8471	ADS8401	ADS8411		
					ADS8405			
16-Bit Pseudo-Bipolar, Fully Diff				ADS8472	ADS8402	ADS8412		
					ADS8406			
14-Bit Pseudo-Diff					ADS7890 (s)		ADS7891	
12-Bit Pseudo-Diff				ADS7886		ADS7883		ADS7881



Please be aware that an important notice concerning availability, standard warranty, and use in critical applications of Texas Instruments semiconductor products and disclaimers thereto appears at the end of this data sheet.



These devices have limited built-in ESD protection. The leads should be shorted together or the device placed in conductive foam during storage or handling to prevent electrostatic damage to the MOS gates.

**ORDERING INFORMATION<sup>(1)</sup>**

MODEL	MAXIMUM INTEGRAL LINEARITY (LSB)	MAXIMUM DIFFERENTIAL LINEARITY (LSB)	NO MISSING CODES RESOLUTION (BIT)	PACKAGE TYPE	PACKAGE DESIGNATOR	TEMPERATURE RANGE	ORDERING INFORMATION	TRANSPORT MEDIA QTY.
ADS8481I	±5	-1 to +2.5	18	7x7 48 Pin QFN	RGZ	-40°C to 85°C	ADS8482IRGZT	Tape and reel 250
							ADS8481IRGZR	Tape and reel 1000
ADS8481IB	±3.5	-1 to +1.5	18	7x7 48 Pin QFN	RGZ	-40°C to 85°C	ADS8481IBRGZT	Tape and reel 250
							ADS8481IBRGZR	Tape and reel 1000

(1) For the most current specifications and package information, refer to our website at [www.ti.com](http://www.ti.com).

**ABSOLUTE MAXIMUM RATINGS<sup>(1)</sup>**

over operating free-air temperature range (unless otherwise noted)

		VALUE	UNIT
Voltage	+IN to AGND	-0.4 to +VA + 0.1	V
	-IN to AGND	-0.4 to 0.5	V
	+VA to AGND	-0.3 to 7	V
	+VBD to BDGND	-0.3 to 7	V
	+VA to +VBD	-0.3 to 2.55	V
Digital input voltage to BDGND		-0.3 to +VBD + 0.3	V
Digital output voltage to BDGND		-0.3 to +VBD + 0.3	V
T <sub>A</sub>	Operating free-air temperature range	-40 to 85	°C
T <sub>stg</sub>	Storage temperature range	-65 to 150	°C
Junction temperature (T <sub>J</sub> max)		150	°C
QFN package	Power dissipation	(T <sub>J</sub> Max - T <sub>A</sub> )/θ <sub>JA</sub>	
	θ <sub>JA</sub> thermal impedance	22	°C/W
Lead temperature, soldering	Vapor phase (60 sec)	215	°C
	Infrared (15 sec)	220	°C

(1) Stresses beyond those listed under *absolute maximum ratings* may cause permanent damage to the device. These are stress ratings only, and functional operation of the device at these or any other conditions beyond those indicated under *recommended operating conditions* is not implied. Exposure to absolute-maximum-rated conditions for extended periods may affect device reliability.

**SPECIFICATIONS**
 $T_A = -40^{\circ}\text{C}$  to  $85^{\circ}\text{C}$ ,  $+V_A = 5\text{ V}$ ,  $+V_{BD} = 3\text{ V}$  or  $5\text{ V}$ ,  $V_{ref} = 4.096\text{ V}$ ,  $f_{SAMPLE} = 1\text{ MSPS}$  (unless otherwise noted)

PARAMETER		TEST CONDITIONS	MIN	TYP	MAX	UNIT	
<b>ANALOG INPUT</b>							
Full-scale input voltage <sup>(1)</sup>		+IN – (–IN)	0		$V_{ref}$	V	
Absolute input voltage		+IN	–0.2		$V_{ref} + 0.2$	V	
		–IN	–0.2		0.2		
Input capacitance				65		pF	
Input leakage current				1		nA	
<b>SYSTEM PERFORMANCE</b>							
Resolution			18			Bits	
No missing codes		ADS8481I	18	18		Bits	
		ADS8481IB	18				
Integral linearity <sup>(2)(3)</sup>		ADS8481I	–5	–1.5/+1.9	5	LSB (18 bit)	
		ADS8481IB	–3.5	–1.5/+1.9	3.5		
Differential linearity		ADS8481I	–1	–0.5/+0.7	2.5	LSB (18 bit)	
		ADS8481IB	–1	–0.5/+0.7	1.5		
Offset error <sup>(4)</sup>		ADS8481I	–0.5	±0.1	0.5	mV	
		ADS8481IB	–0.5	±0.1	0.5		
Offset error temperature drift				±0.2		ppm/°C	
Gain error <sup>(4)(5)</sup>		ADS8481I	$V_{ref} = 4.096\text{ V}$	–0.075	±0.05	0.075	%FS
		ADS8481IB	$V_{ref} = 4.096\text{ V}$	–0.075	±0.05	0.075	
Gain error temperature drift				±0.6		ppm/°C	
Noise				30		μV RMS	
Power supply rejection ratio		At 3FFFFh output code		60		dB	
<b>SAMPLING DYNAMICS</b>							
Conversion time				650	710	ns	
Acquisition time			250			ns	
Throughput rate					1	MHz	
Aperture delay				4		ns	
Aperture jitter				5		ps	
Step response				150		ns	
Over voltage recovery				150		ns	

(1) Ideal input span, does not include gain or offset error.

(2) LSB means least significant bit

(3) This is endpoint INL, not best fit.

(4) Measured relative to an ideal full-scale input [+IN – (–IN)] of 4.096 V

(5) This specification does not include the internal reference voltage error and drift.

**SPECIFICATIONS (Continued)**

$T_A = -40^\circ\text{C}$  to  $85^\circ\text{C}$ ,  $+V_A = 5\text{ V}$ ,  $+V_{BD} = 3\text{ V}$  or  $5\text{ V}$ ,  $V_{ref} = 4.096\text{ V}$ ,  $f_{SAMPLE} = 1\text{ MSPS}$  (unless otherwise noted)

PARAMETER		TEST CONDITIONS	MIN	TYP	MAX	UNIT
<b>DYNAMIC CHARACTERISTICS</b>						
Total harmonic distortion (THD) <sup>(1)</sup>	ADS8481I	$V_{IN} = 4 V_{pp}$ at 1 kHz		-110		dB
	ADS8481IB			-112		
	ADS8481I	$V_{IN} = 4 V_{pp}$ at 10 kHz		-106		
	ADS8481IB			-108		
	ADS8481I	$V_{IN} = 4 V_{pp}$ at 100 kHz		-98		
	ADS8481IB			-99		
Signal to noise ratio (SNR) <sup>(1)</sup>	ADS8481I	$V_{IN} = 4 V_{pp}$ at 1 kHz		92		dB
	ADS8481IB			94		
	ADS8481I	$V_{IN} = 4 V_{pp}$ at 10 kHz		91		
	ADS8481IB			93		
	ADS8481I	$V_{IN} = 4 V_{pp}$ at 100 kHz		90		
	ADS8481IB			92		
Signal to noise + distortion (SINAD) <sup>(1)</sup>	ADS8481I	$V_{IN} = 4 V_{pp}$ at 1 kHz		91		dB
	ADS8481IB			93		
	ADS8481I	$V_{IN} = 4 V_{pp}$ at 10 kHz		90		
	ADS8481IB			92		
	ADS8481I	$V_{IN} = 4 V_{pp}$ at 100 kHz		89		
	ADS8481IB			91		
Spurious free dynamic range (SFDR) <sup>(1)</sup>	ADS8481I	$V_{IN} = 4 V_{pp}$ at 1 kHz		110		dB
	ADS8481IB			112		
	ADS8481I	$V_{IN} = 4 V_{pp}$ at 10 kHz		108		
	ADS8481IB			107		
	ADS8481I	$V_{IN} = 4 V_{pp}$ at 100 kHz		98		
	ADS8481IB			98		
-3dB Small signal bandwidth				15		MHz
<b>VOLTAGE REFERENCE INPUT</b>						
Reference voltage at REFIN, $V_{ref}$			3.0	4.096	4.2	V
Reference resistance <sup>(2)</sup>				500		k $\Omega$
Reference current drain		$f_s = 1\text{ MHz}$			1	mA

(1) Calculated on the first nine harmonics of the input frequency.

(2) Can vary  $\pm 20\%$

**SPECIFICATIONS (Continued)**
 $T_A = -40^{\circ}\text{C}$  to  $85^{\circ}\text{C}$ ,  $+VA = 5\text{ V}$ ,  $+VBD = 3\text{ V}$  or  $5\text{ V}$ ,  $V_{\text{ref}} = 4.096\text{ V}$ ,  $f_{\text{SAMPLE}} = 1\text{ MSPS}$  (unless otherwise noted)

PARAMETER		TEST CONDITIONS	MIN	TYP	MAX	UNIT
<b>INTERNAL REFERENCE OUTPUT</b>						
Internal reference start-up time		From 95% (+VA), with 1- $\mu\text{F}$ storage capacitor			120	ms
Reference voltage range, $V_{\text{ref}}$		$I_O = 0\text{ A}$	4.081	4.096	4.111	V
Source current		Static load			10	$\mu\text{A}$
Line regulation		$+VA = 4.75\text{ V}$ to $5.25\text{ V}$		60		$\mu\text{V}$
Drift		$I_O = 0\text{ A}$		$\pm 6$		PPM/C
<b>DIGITAL INPUT/OUTPUT</b>						
Logic family – CMOS						
Logic level	$V_{\text{IH}}$	$I_{\text{IH}} = 5\text{ }\mu\text{A}$	$+V_{\text{BD}} - 1$		$+V_{\text{BD}} + 0.3$	V
	$V_{\text{IL}}$	$I_{\text{IL}} = 5\text{ }\mu\text{A}$	-0.3		0.8	
	$V_{\text{OH}}$	$I_{\text{OH}} = 2\text{ TTL loads}$	$+V_{\text{BD}} - 0.6$			
	$V_{\text{OL}}$	$I_{\text{OL}} = 2\text{ TTL loads}$			0.4	
Data format – Straight Binary						
<b>POWER SUPPLY REQUIREMENTS</b>						
Power supply voltage	+VBD		2.7	3.3	5.25	V
	+VA		4.75	5	5.25	V
Supply current <sup>(1)</sup>		$f_s = 1\text{ MHz}$		44	48	mA
Power dissipation <sup>(1)</sup>		$f_s = 1\text{ MHz}$		220	240	mW
<b>TEMPERATURE RANGE</b>						
Operating free-air			-40		85	$^{\circ}\text{C}$

(1) This includes only +VA current. +VBD current is typical 1 mA with 5 pF load capacitance on all output pins.

**TIMING CHARACTERISTICS**

All specifications typical at -40°C to 85°C, +VA = +VBD = 5 V <sup>(1)(2)(3)</sup>

PARAMETER		MIN	TYP	MAX	UNIT
t <sub>(CONV)</sub>	Conversion time			710	ns
t <sub>(ACQ)</sub>	Acquisition time	250			ns
t <sub>(HOLD)</sub>	Sample capacitor hold time			25	ns
t <sub>pd1</sub>	$\overline{\text{CONVST}}$ low to BUSY high			40	ns
t <sub>pd2</sub>	Propagation delay time, end of conversion to BUSY low			15	ns
t <sub>pd3</sub>	Propagation delay time, start of convert state to rising edge of BUSY			15	ns
t <sub>w1</sub>	Pulse duration, $\overline{\text{CONVST}}$ low	40			ns
t <sub>su1</sub>	Setup time, $\overline{\text{CS}}$ low to $\overline{\text{CONVST}}$ low	20			ns
t <sub>w2</sub>	Pulse duration, $\overline{\text{CONVST}}$ high	20			ns
	$\overline{\text{CONVST}}$ falling edge jitter			10	ps
t <sub>w3</sub>	Pulse duration, BUSY signal low	t <sub>(ACQ)</sub> min			ns
t <sub>w4</sub>	Pulse duration, BUSY signal high			710	ns
t <sub>h1</sub>	Hold time, first data bus transition ( $\overline{\text{RD}}$ low, or $\overline{\text{CS}}$ low for read cycle, or BYTE or BUS18/16 input changes) after $\overline{\text{CONVST}}$ low	40			ns
t <sub>d1</sub>	Delay time, $\overline{\text{CS}}$ low to $\overline{\text{RD}}$ low	0			ns
t <sub>su2</sub>	Setup time, $\overline{\text{RD}}$ high to $\overline{\text{CS}}$ high	0			ns
t <sub>w5</sub>	Pulse duration, $\overline{\text{RD}}$ low	50			ns
t <sub>en</sub>	Enable time, $\overline{\text{RD}}$ low (or $\overline{\text{CS}}$ low for read cycle) to data valid			20	ns
t <sub>d2</sub>	Delay time, data hold from $\overline{\text{RD}}$ high	5			ns
t <sub>d3</sub>	Delay time, BUS18/16 or BYTE rising edge or falling edge to data valid	10		20	ns
t <sub>w6</sub>	Pulse duration, $\overline{\text{RD}}$ high	20			ns
t <sub>w7</sub>	Pulse duration, $\overline{\text{CS}}$ high	20			ns
t <sub>h2</sub>	Hold time, last $\overline{\text{RD}}$ (or $\overline{\text{CS}}$ for read cycle ) rising edge to $\overline{\text{CONVST}}$ falling edge	50			ns
t <sub>pd4</sub>	Propagation delay time, BUSY falling edge to next $\overline{\text{RD}}$ (or $\overline{\text{CS}}$ for read cycle) falling edge	0			ns
t <sub>d4</sub>	Delay time, BYTE edge to BUS18/16 edge skew	0			ns
t <sub>su3</sub>	Setup time, BYTE or BUS18/16 transition to $\overline{\text{RD}}$ falling edge	10			ns
t <sub>h3</sub>	Hold time, BYTE or BUS18/16 transition to $\overline{\text{RD}}$ falling edge	10			ns
t <sub>dis</sub>	Disable time, $\overline{\text{RD}}$ high ( $\overline{\text{CS}}$ high for read cycle) to 3-stated data bus			20	ns
t <sub>d5</sub>	Delay time, BUSY low to MSB data valid delay			0	ns
t <sub>d6</sub>	Delay time, $\overline{\text{CS}}$ rising edge to BUSY falling edge	50			ns
t <sub>d7</sub>	Delay time, BUSY falling edge to $\overline{\text{CS}}$ rising edge	50			ns
t <sub>su5</sub>	BYTE transition setup time, from BYTE transition to next BYTE transition, or BUS18/16 transition setup time, from BUS18/16 to next BUS18/16.	50			ns
t <sub>su(ABORT)</sub>	Setup time from the falling edge of $\overline{\text{CONVST}}$ (used to start the valid conversion) to the next falling edge of $\overline{\text{CONVST}}$ (when CS = 0 and $\overline{\text{CONVST}}$ are used to abort) or to the next falling edge of $\overline{\text{CS}}$ (when $\overline{\text{CS}}$ is used to abort).	60		610	ns

- (1) All input signals are specified with t<sub>r</sub> = t<sub>f</sub> = 5 ns (10% to 90% of +VBD) and timed from a voltage level of (V<sub>IL</sub> + V<sub>IH</sub>)/2.
- (2) See timing diagrams.
- (3) All timing are measured with 20-pF equivalent loads on all data bits and BUSY pins.

## TIMING CHARACTERISTICS

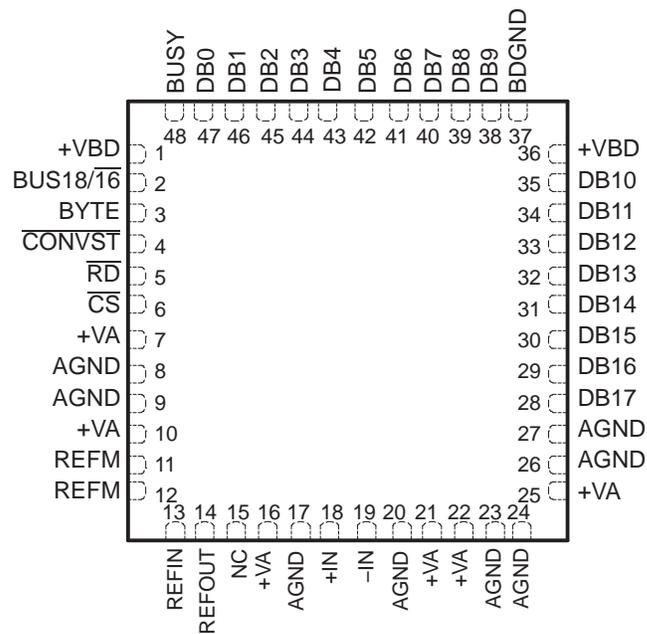
All specifications typical at  $-40^{\circ}\text{C}$  to  $85^{\circ}\text{C}$ ,  $+V_A = 5\text{ V}$   $+V_{BD} = 3\text{ V}$  <sup>(1)(2)(3)</sup>

PARAMETER		MIN	TYP	MAX	UNIT
$t_{(\text{CONV})}$	Conversion time			710	ns
$t_{(\text{ACQ})}$	Acquisition time	250			ns
$t_{(\text{HOLD})}$	Sample capacitor hold time			25	ns
$t_{\text{pd1}}$	$\overline{\text{CONVST}}$ low to BUSY high			40	ns
$t_{\text{pd2}}$	Propagation delay time, end of conversion to BUSY low			25	ns
$t_{\text{pd3}}$	Propagation delay time, start of convert state to rising edge of BUSY			25	ns
$t_{\text{w1}}$	Pulse duration, $\overline{\text{CONVST}}$ low	40			ns
$t_{\text{su1}}$	Setup time, $\overline{\text{CS}}$ low to $\overline{\text{CONVST}}$ low	20			ns
$t_{\text{w2}}$	Pulse duration, $\overline{\text{CONVST}}$ high	20			ns
	$\overline{\text{CONVST}}$ falling edge jitter			10	ps
$t_{\text{w3}}$	Pulse duration, BUSY signal low	$t_{(\text{ACQ})\text{min}}$			ns
$t_{\text{w4}}$	Pulse duration, BUSY signal high			710	ns
$t_{\text{h1}}$	Hold time, first data bus transition ( $\overline{\text{RD}}$ low, or $\overline{\text{CS}}$ low for read cycle, or BYTE or BUS18/16 input changes) after $\overline{\text{CONVST}}$ low	40			ns
$t_{\text{d1}}$	Delay time, $\overline{\text{CS}}$ low to $\overline{\text{RD}}$ low	0			ns
$t_{\text{su2}}$	Setup time, $\overline{\text{RD}}$ high to $\overline{\text{CS}}$ high	0			ns
$t_{\text{w5}}$	Pulse duration, $\overline{\text{RD}}$ low	50			ns
$t_{\text{en}}$	Enable time, $\overline{\text{RD}}$ low (or $\overline{\text{CS}}$ low for read cycle) to data valid			30	ns
$t_{\text{d2}}$	Delay time, data hold from $\overline{\text{RD}}$ high	5			ns
$t_{\text{d3}}$	Delay time, BUS18/16 or BYTE rising edge or falling edge to data valid	10		30	ns
$t_{\text{w6}}$	Pulse duration, $\overline{\text{RD}}$ high	20			ns
$t_{\text{w7}}$	Pulse duration, $\overline{\text{CS}}$ high	20			ns
$t_{\text{h2}}$	Hold time, last $\overline{\text{RD}}$ (or $\overline{\text{CS}}$ for read cycle ) rising edge to $\overline{\text{CONVST}}$ falling edge	50			ns
$t_{\text{pd4}}$	Propagation delay time, BUSY falling edge to next $\overline{\text{RD}}$ (or $\overline{\text{CS}}$ for read cycle) falling edge	0			ns
$t_{\text{d4}}$	Delay time, BYTE edge to BUS18/16 edge skew	0			ns
$t_{\text{su3}}$	Setup time, BYTE or BUS18/16 transition to $\overline{\text{RD}}$ falling edge	10			ns
$t_{\text{h3}}$	Hold time, BYTE or BUS18/16 transition to $\overline{\text{RD}}$ falling edge	10			ns
$t_{\text{dis}}$	Disable time, $\overline{\text{RD}}$ high ( $\overline{\text{CS}}$ high for read cycle) to 3-stated data bus			30	ns
$t_{\text{d5}}$	Delay time, BUSY low to MSB data valid delay			0	ns
$t_{\text{d6}}$	Delay time, $\overline{\text{CS}}$ rising edge to BUSY falling edge	50			ns
$t_{\text{d7}}$	Delay time, BUSY falling edge to $\overline{\text{CS}}$ rising edge	50			ns
$t_{\text{su5}}$	BYTE transition setup time, from BYTE transition to next BYTE transition, or BUS18/16 transition setup time, from BUS18/16 to next BUS18/16.	50			ns
$t_{\text{su(ABORT)}}$	Setup time from the falling edge of $\overline{\text{CONVST}}$ (used to start the valid conversion) to the next falling edge of $\overline{\text{CONVST}}$ (when $\text{CS} = 0$ and $\overline{\text{CONVST}}$ are used to abort) or to the next falling edge of $\overline{\text{CS}}$ (when $\overline{\text{CS}}$ is used to abort).	70		620	ns

- (1) All input signals are specified with  $t_r = t_f = 5\text{ ns}$  (10% to 90% of  $+V_{BD}$ ) and timed from a voltage level of  $(V_{IL} + V_{IH})/2$ .
- (2) See timing diagrams.
- (3) All timing are measured with 20-pF equivalent loads on all data bits and BUSY pins.

**PIN ASSIGNMENTS**

**RGZ PACKAGE  
(TOP VIEW)**



NC – No internal connection

NOTE: The package thermal pad must be soldered to the printed circuit board for thermal and mechanical performance.

## PIN ASSIGNMENTS (continued)

### TERMINAL FUNCTIONS

NAME	NO RGZ	I/O	DESCRIPTION					
AGND	8, 9, 17, 20, 23, 24, 26, 27	–	Analog ground					
BDGND	37	–	Digital ground for bus interface digital supply					
BUSY	48	O	Status output. High when a conversion is in progress.					
BUS18/ $\overline{16}$	2	I	Bus size select input. Used for selecting 18-bit or 16-bit wide bus transfer. 0: Data bits output on the 18-bit data bus pins DB[17:0]. 1: Last two data bits D[1:0] from 18-bit wide bus output on: a) the low byte pins DB[9:2] if BYTE = 0 b) the high byte pins DB[17:10] if BYTE = 1					
BYTE	3	I	Byte select input. Used for 8-bit bus reading. 0: No fold back 1: Low byte D[9:2] of the 16 most significant bits is folded back to high byte of the 16 most significant pins DB[17:10].					
$\overline{\text{CONVST}}$	4	I	Convert start. The falling edge of this input ends the acquisition period and starts the hold period.					
$\overline{\text{CS}}$	6	I	Chip select. The falling edge of this input starts the acquisition period.					
Data Bus			8-BIT BUS			16-BIT BUS		18-BIT BUS
			BYTE = 0	BYTE = 1	BYTE = 1	BYTE = 0	BYTE = 0	BYTE = 0
			BUS18/ $\overline{16}$ = 0	BUS18/ $\overline{16}$ = 0	BUS18/ $\overline{16}$ = 1	BUS18/ $\overline{16}$ = 0	BUS18/ $\overline{16}$ = 1	BUS18/ $\overline{16}$ = 0
DB17	28	O	D17 (MSB)	D9	All ones	D17 (MSB)	All ones	D17 (MSB)
DB16	29	O	D16	D8	All ones	D16	All ones	D16
DB15	30	O	D15	D7	All ones	D15	All ones	D15
DB14	31	O	D14	D6	All ones	D14	All ones	D14
DB13	32	O	D13	D5	All ones	D13	All ones	D13
DB12	33	O	D12	D4	All ones	D12	All ones	D12
DB11	34	O	D11	D3	D1	D11	All ones	D11
DB10	35	O	D10	D2	D0 (LSB)	D10	All ones	D10
DB9	38	O	D9	All ones	All ones	D9	All ones	D9
DB8	39	O	D8	All ones	All ones	D8	All ones	D8
DB7	40	O	D7	All ones	All ones	D7	All ones	D7
DB6	41	O	D6	All ones	All ones	D6	All ones	D6
DB5	42	O	D5	All ones	All ones	D5	All ones	D5
DB4	43	O	D4	All ones	All ones	D4	All ones	D4
DB3	44	O	D3	All ones	All ones	D3	D1	D3
DB2	45	O	D2	All ones	All ones	D2	D0 (LSB)	D2
DB1	46	O	D1	All ones	All ones	D1	All ones	D1
DB0	47	O	D0 (LSB)	All ones	All ones	D0 (LSB)	All ones	D0 (LSB)
–IN	19	I	Inverting input channel					
+IN	18	I	Noninverting input channel					
NC	15		No connection					
REFIN	13	I	Reference input					
REFOUT	14	O	Reference output. Add 1- $\mu$ F capacitor between the REFOUT pin and REFM pin when internal reference is used.					
REFM	11, 12	I	Reference ground					
$\overline{\text{RD}}$	5	I	Synchronization pulse for the parallel output. When $\overline{\text{CS}}$ is low, this serves as output enable and puts the previous conversion results on the bus.					
+VA	7, 10, 16, 21, 22, 25	–	Analog power supplies, 5-V DC					
+VBD	1, 36	–	Digital power supply for bus					

TYPICAL CHARACTERISTICS

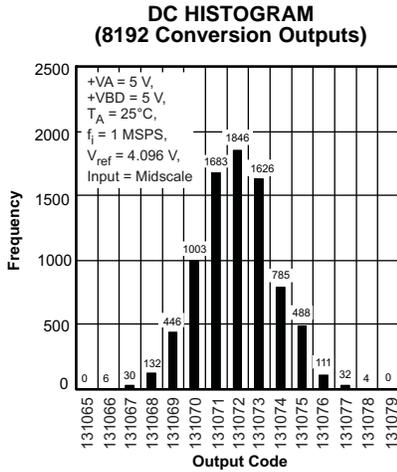


Figure 1.

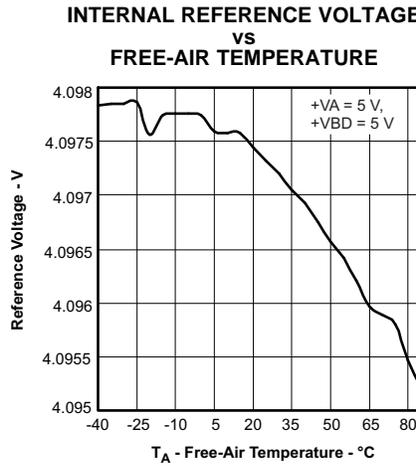


Figure 2.

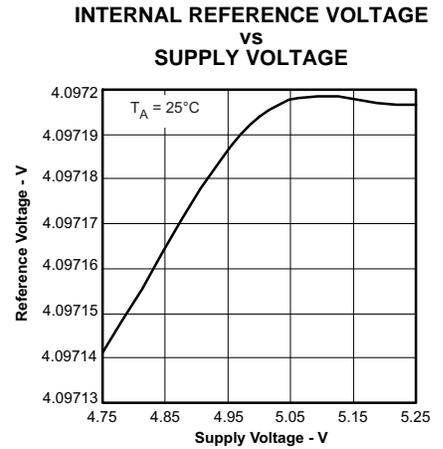


Figure 3.

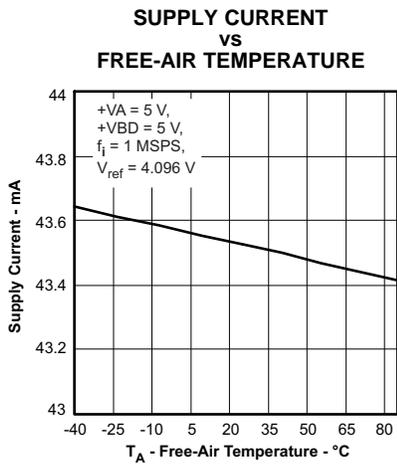


Figure 4.

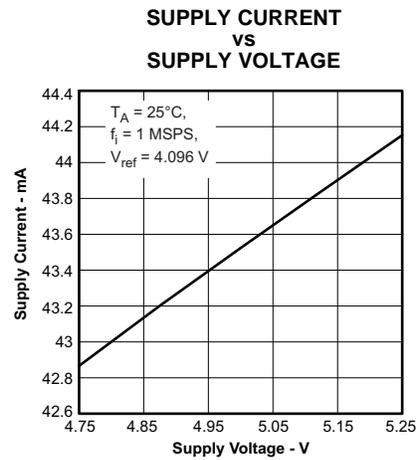


Figure 5.

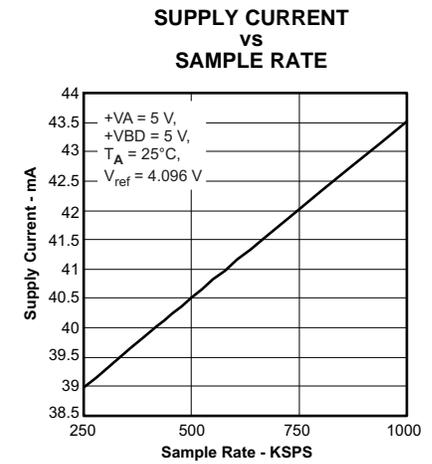


Figure 6.

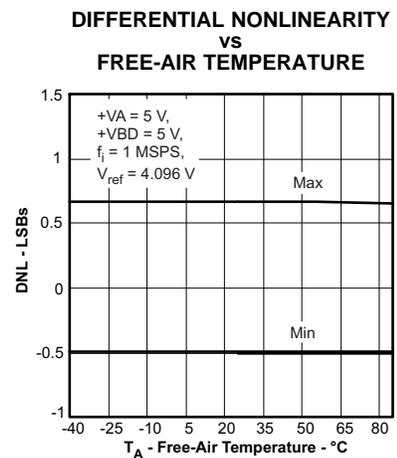


Figure 7.

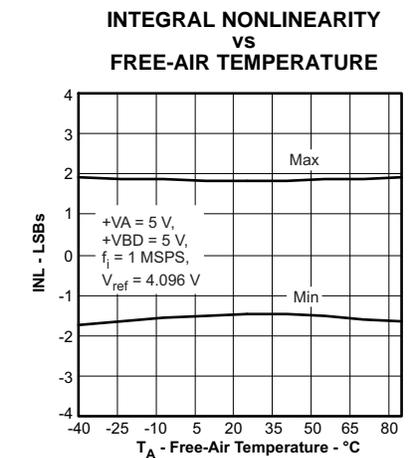


Figure 8.

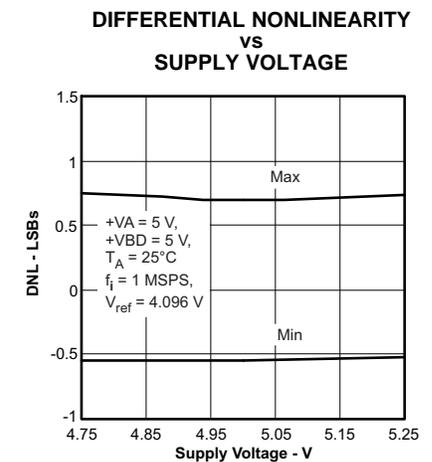


Figure 9.

**TYPICAL CHARACTERISTICS (continued)**

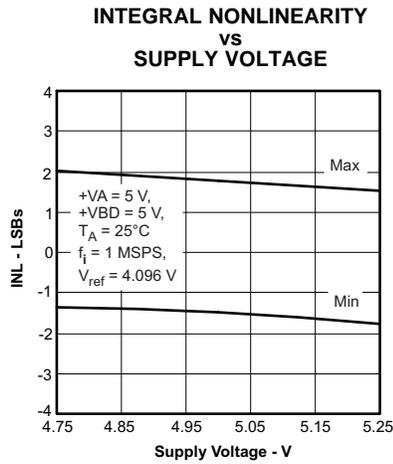


Figure 10.

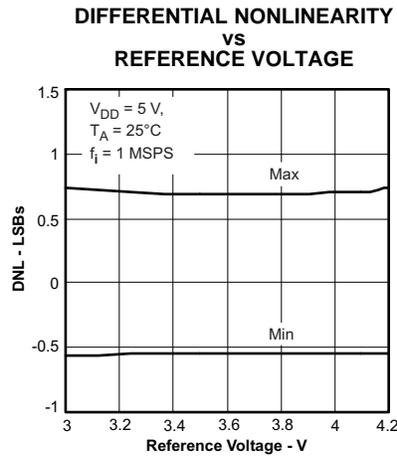


Figure 11.

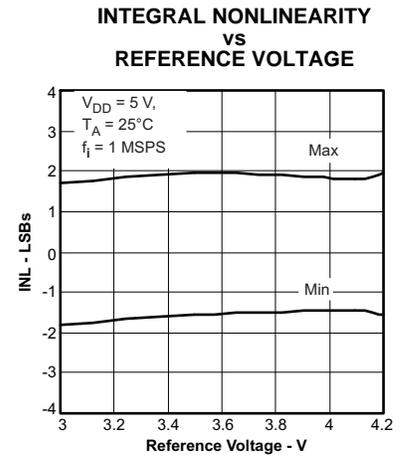


Figure 12.

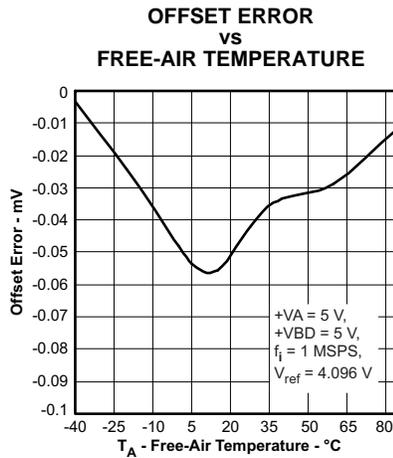


Figure 13.

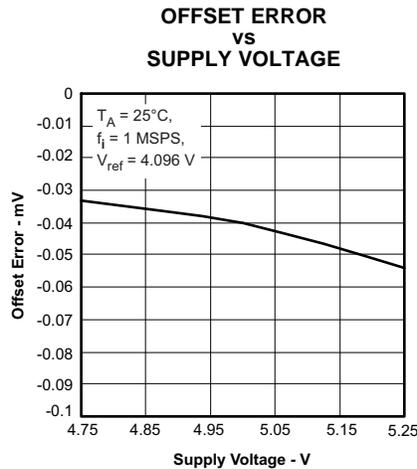


Figure 14.

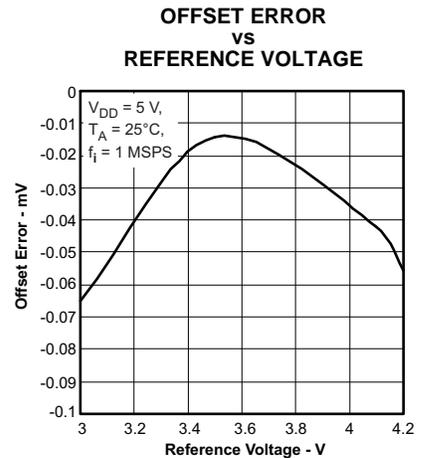


Figure 15.

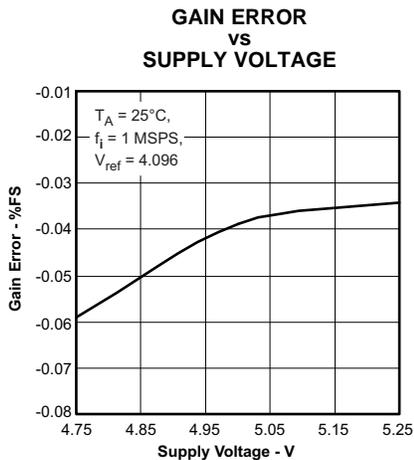


Figure 16.

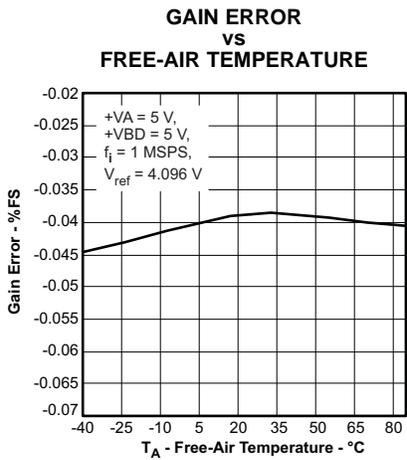


Figure 17.

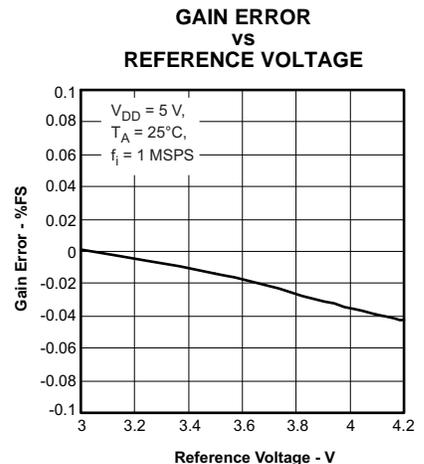


Figure 18.

**TYPICAL CHARACTERISTICS (continued)**

**OFFSET ERROR TEMPERATURE DRIFT DISTRIBUTION (25 Samples)**

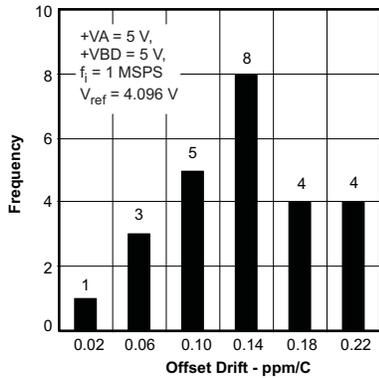


Figure 19.

**GAIN ERROR TEMPERATURE DRIFT DISTRIBUTION (25 Samples)**

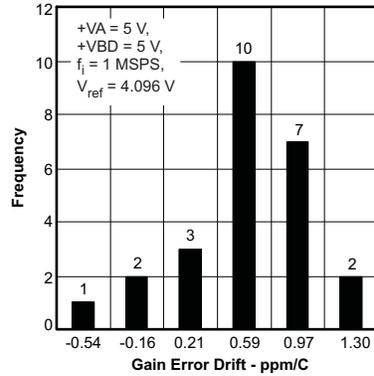


Figure 20.

**TOTAL HARMONIC DISTORTION vs REFERENCE VOLTAGE**

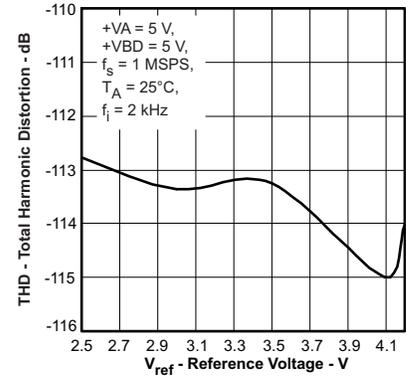


Figure 21.

**SIGNAL-TO-NOISE RATIO vs REFERENCE VOLTAGE**

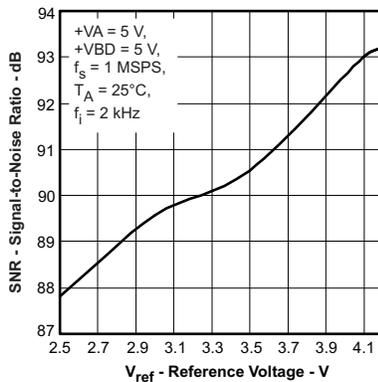


Figure 22.

**SIGNAL-TO-NOISE + DISTORTION vs REFERENCE VOLTAGE**

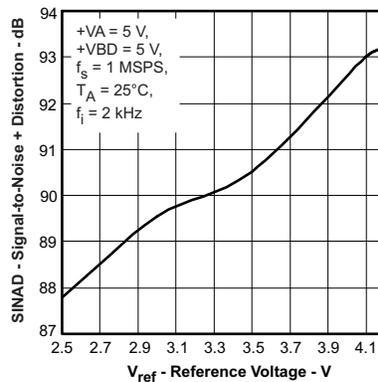


Figure 23.

**TOTAL HARMONIC DISTORTION vs FREE-AIR TEMPERATURE**

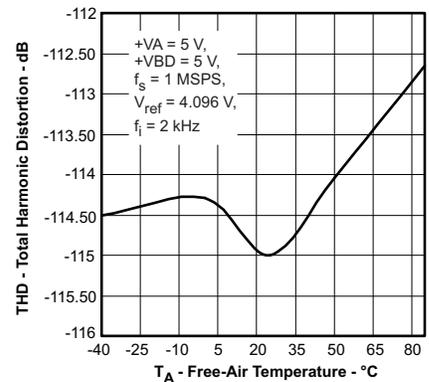


Figure 24.

**SPURIOUS FREE DYNAMIC RANGE vs FREE-AIR TEMPERATURE**

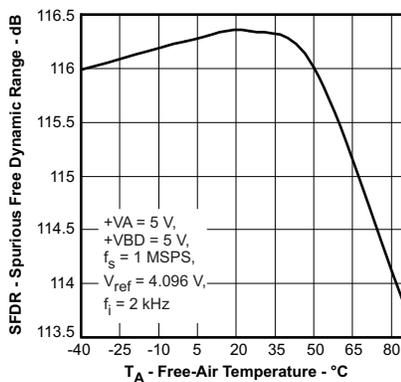


Figure 25.

**SIGNAL-TO-NOISE RATIO vs FREE-AIR TEMPERATURE**

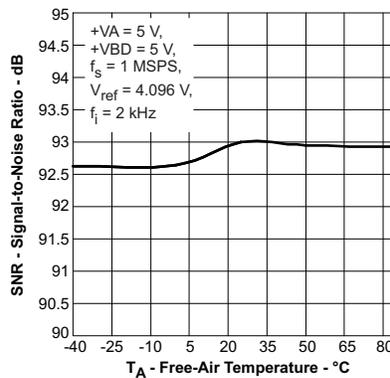


Figure 26.

**SIGNAL-TO-NOISE + DISTORTION vs FREE-AIR TEMPERATURE**

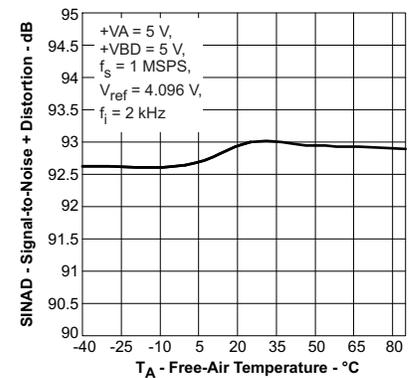


Figure 27.

**TYPICAL CHARACTERISTICS (continued)**

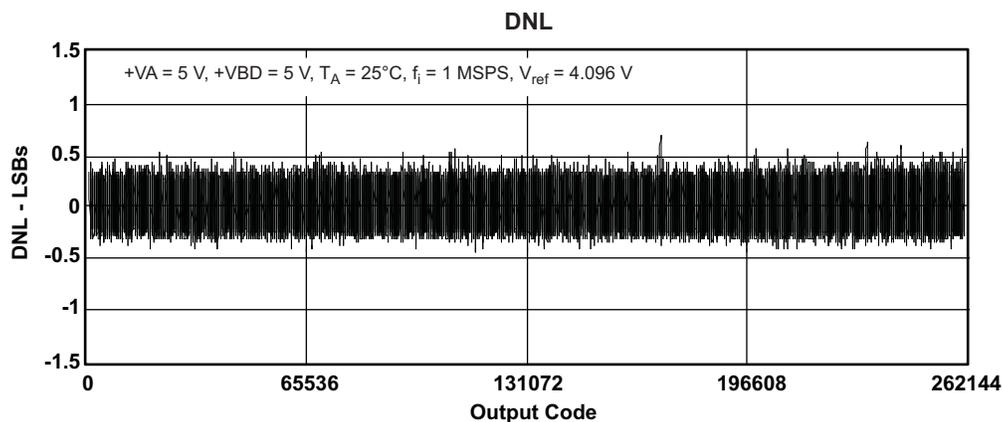


Figure 28.

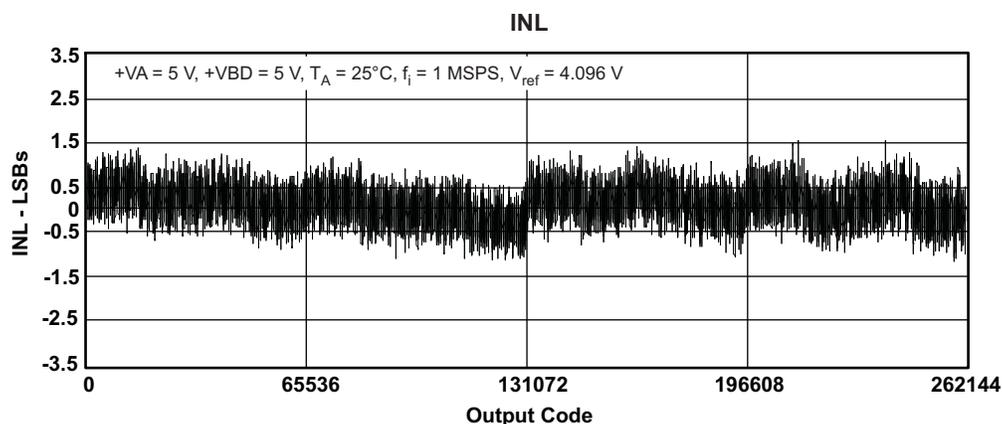


Figure 29.

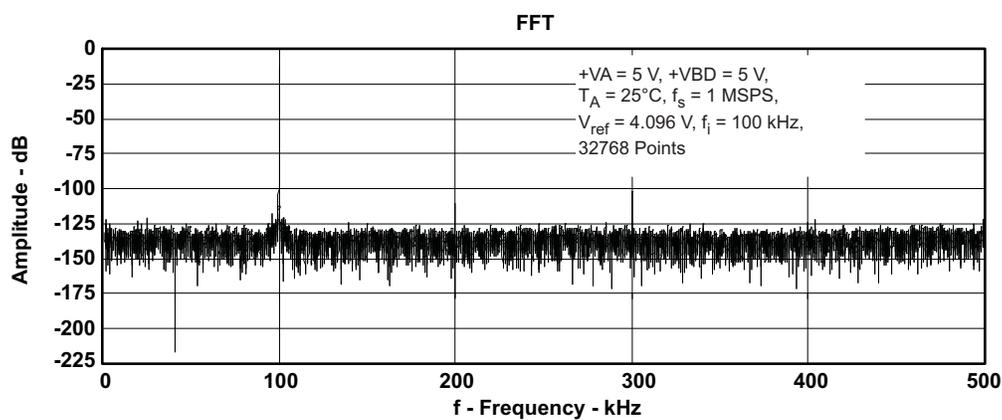
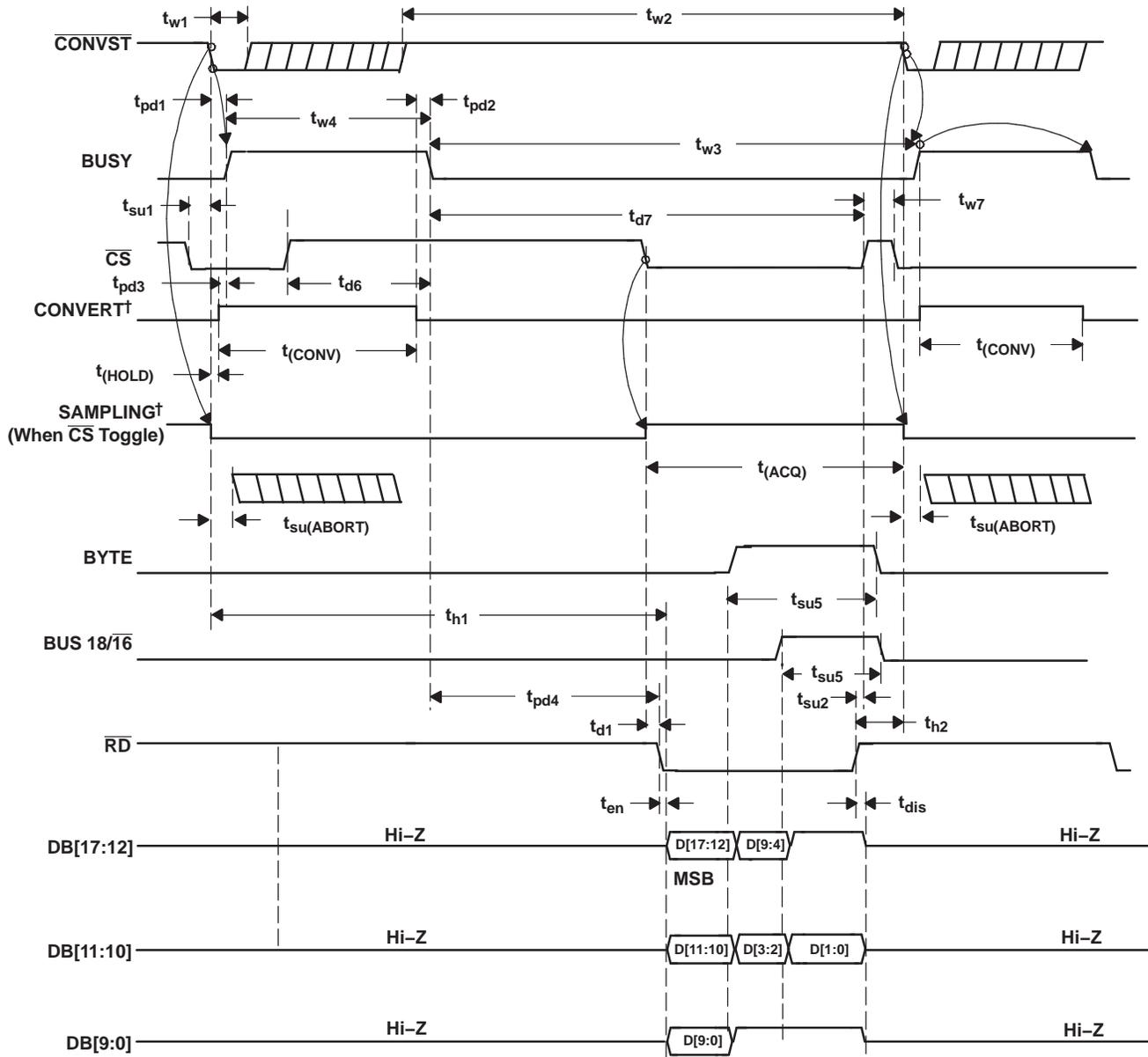


Figure 30.

**TYPICAL CHARACTERISTICS (continued)**

**TIMING DIAGRAMS**



†Signal internal to device

**Figure 31. Timing for Conversion and Acquisition Cycles With  $\overline{CS}$  and  $\overline{RD}$  Toggling**

TYPICAL CHARACTERISTICS (continued)

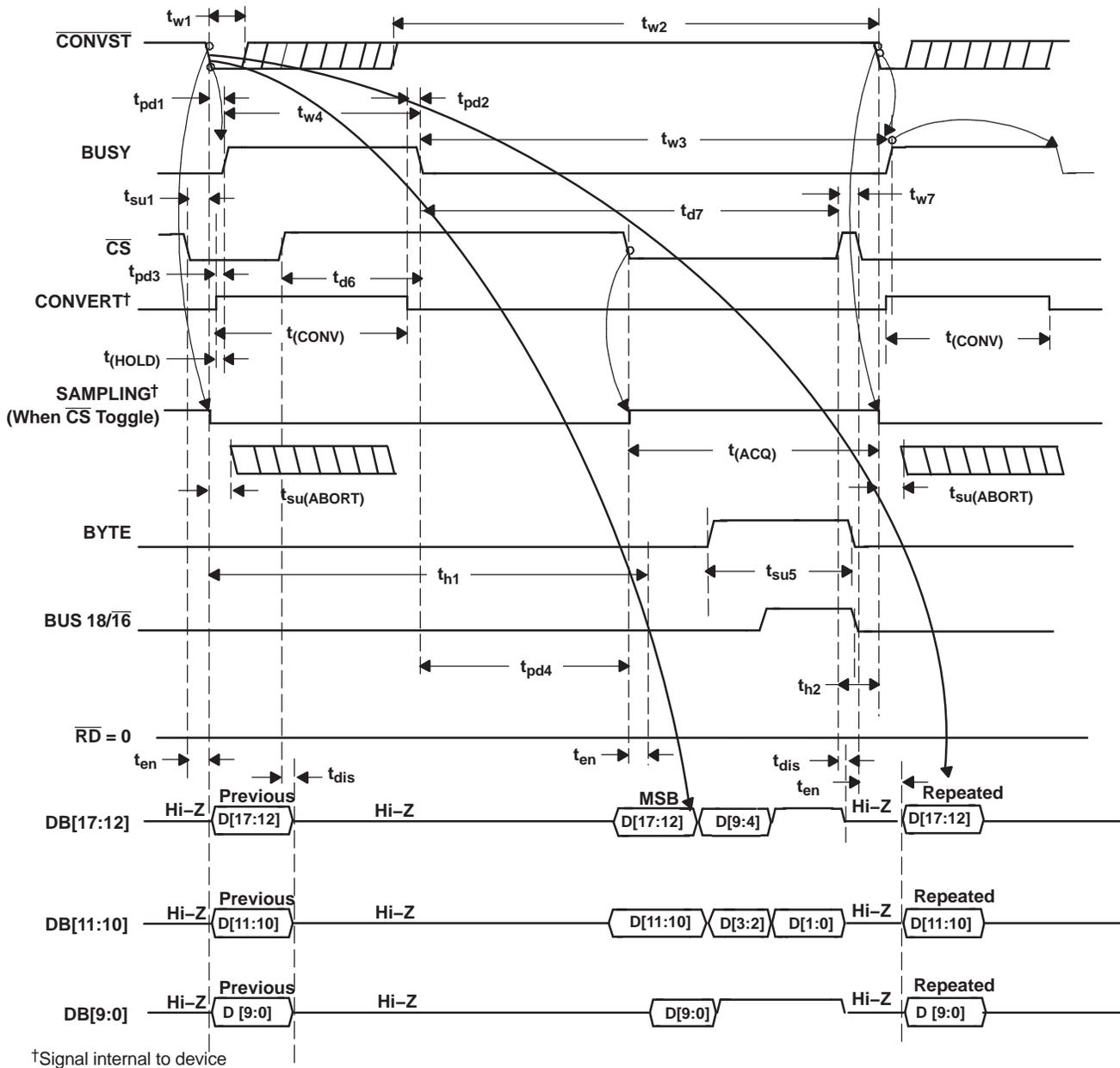
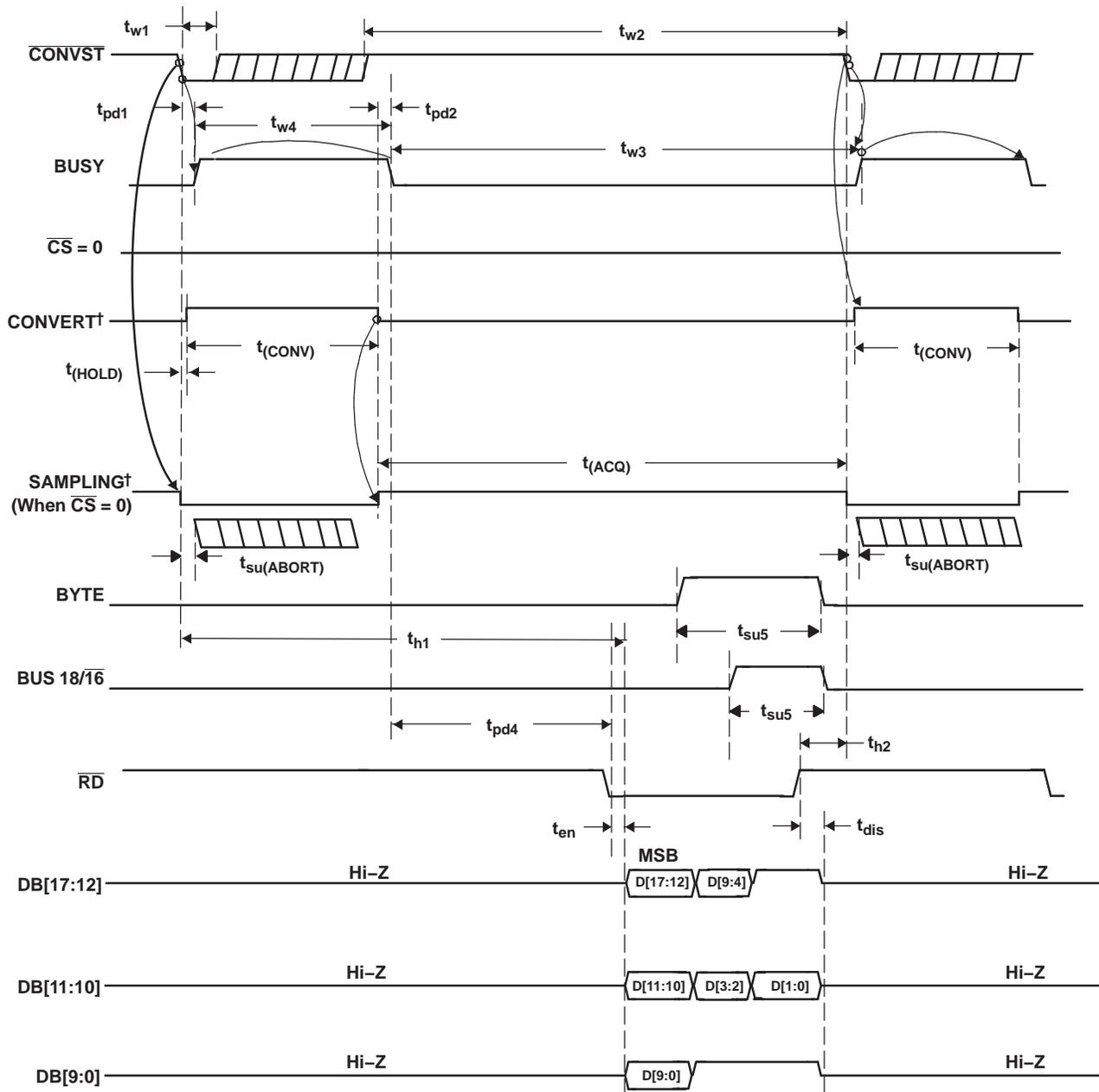


Figure 32. Timing for Conversion and Acquisition Cycles With  $\overline{CS}$  Toggling,  $\overline{RD}$  Tied to BDGND

TYPICAL CHARACTERISTICS (continued)



†Signal internal to device

Figure 33. Timing for Conversion and Acquisition Cycles With CS Tied to BDGND, RD Toggling



TYPICAL CHARACTERISTICS (continued)

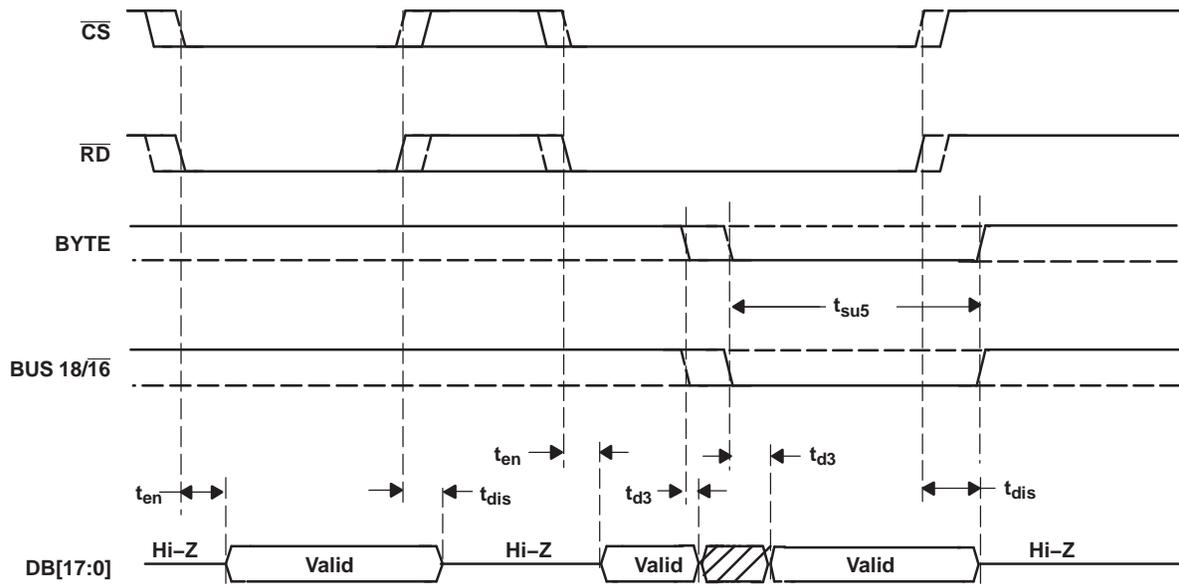


Figure 35. Detailed Timing for Read Cycles



## PRINCIPLES OF OPERATION

The ADS8481 is a high-speed successive approximation register (SAR) analog-to-digital converter (ADC). The architecture is based on charge redistribution which inherently includes a sample/hold function. See [Figure 36](#) for the application circuit for the ADS8481.

The conversion clock is generated internally. The conversion time of 710 ns is capable of sustaining a 1 MHz throughput.

The analog input is provided to two input pins: +IN and -IN. When a conversion is initiated, the differential input on these pins is sampled on the internal capacitor array. While a conversion is in progress, both inputs are disconnected from any internal function.

## REFERENCE

The ADS8481 can operate with an external reference with a range from 3.0 V to 4.2 V. The reference voltage on the input pin #1 (REFIN) of the converter is internally buffered. A clean, low noise, well-decoupled reference voltage on this pin is required to ensure good performance of the converter. A low noise band-gap reference like the REF3240 can be used to drive this pin. A 0.1- $\mu$ F decoupling capacitor is required between REFIN and REFM pins (pin #13 and pin #12) of the converter. This capacitor should be placed as close as possible to the pins of the device. Designers should strive to minimize the routing length of the traces that connect the terminals of the capacitor to the pins of the converter. An RC network can also be used to filter the reference voltage. A 100- $\Omega$  series resistor and a 0.1- $\mu$ F capacitor, which can also serve as the decoupling capacitor can be used to filter the reference voltage.

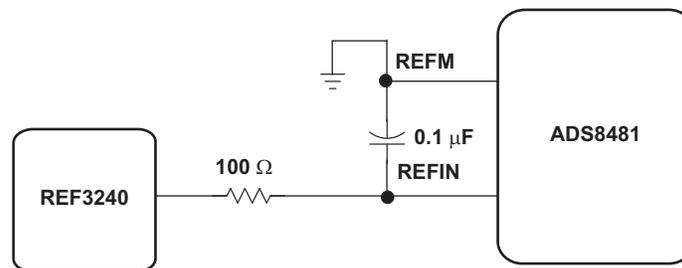


Figure 38. Reference Circuit

The ADS8481 also has limited low pass filtering capability built into the converter. The equivalent circuitry on the REFIN input is as shown in [Figure 39](#).

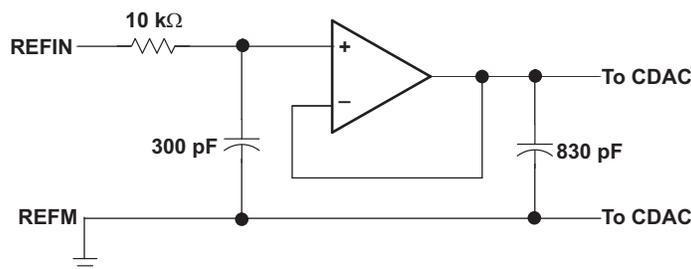


Figure 39. Reference Circuit

The REFM input of the ADS8481 should always be shorted to AGND.

A 4.096-V internal reference is included. When internal reference is used, pin 14 (REFOUT) is connected to pin 13 (REFIN) with a 0.1- $\mu$ F decoupling capacitor and 1-nF storage capacitor between pin 14 (REFOUT) and pins 11 and 12 (REFM) (see [Figure 37](#)). The internal reference of the converter is double buffered. If an external reference is used, the second buffer provides isolation between the external reference and the CDAC. This buffer is also used to recharge all of the capacitors of the CDAC during conversion. Pin 14 (REFOUT) can be left unconnected (floating) if an external reference is used.

## PRINCIPLES OF OPERATION (continued)

### ANALOG INPUT

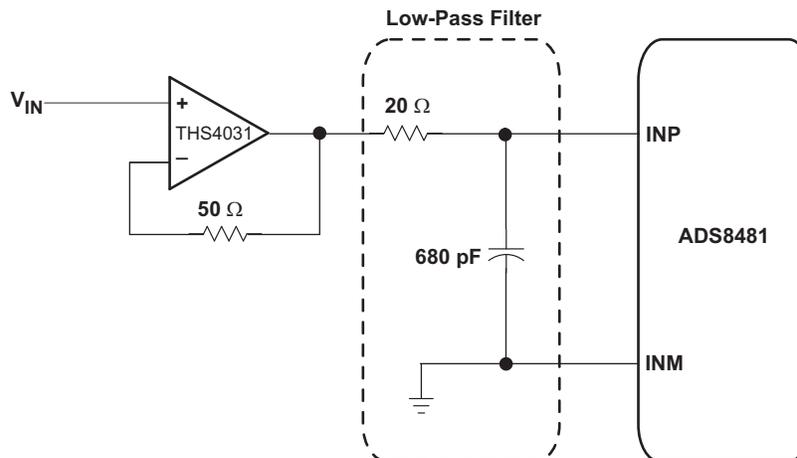
When the converter enters the hold mode, the voltage difference between the +IN and –IN inputs is captured on the internal capacitor array. The voltage on the –IN input is limited between  $-0.2\text{ V}$  and  $0.2\text{ V}$ , allowing the input to reject small signals which are common to both the +IN and –IN inputs. The +IN input has a range of  $-0.2\text{ V}$  to  $V_{\text{ref}} + 0.2\text{ V}$ . The input span [+IN – (–IN)] is limited to  $0\text{ V}$  to  $V_{\text{ref}}$ .

The input current on the analog inputs depends upon a number of factors: sample rate, input voltage, and source impedance. Essentially, the current into the ADS8481 charges the internal capacitor array during the sample period. After this capacitance has been fully charged, there is no further input current. The source of the analog input voltage must be able to charge the input capacitance ( $65\text{ pF}$ ) to an 18-bit settling level within the acquisition time ( $250\text{ ns}$ ) of the device. When the converter goes into the hold mode, the input impedance is greater than  $1\text{ G}\Omega$ .

Care must be taken regarding the absolute analog input voltage. To maintain the linearity of the converter, the +IN and –IN inputs and the span [+IN – (–IN)] must be within the limits specified. Outside of these ranges, the converter's linearity may not meet specifications. To minimize noise, low bandwidth input signals with low-pass filters are used.

Care must be taken to ensure that the output impedance of the sources driving the +IN and –IN inputs are matched. If this is not observed, the two inputs could have different settling times. This may result in offset error, gain error, and linearity error which varies with temperature and input voltage.

The analog input to the converter needs to be driven with a low noise, high-speed op-amp like the THS4031. An RC filter is recommended at the input pins to low-pass filter the noise from the source. A series resistor of  $20\text{ }\Omega$  and a decoupling capacitor of  $680\text{ pF}$  is recommended. The input to the converter is a uni-polar input voltage in the range  $0$  to  $V_{\text{ref}}$ . The THS4031 can be used in the source follower configuration to drive the converter.



**Figure 40. Input Circuit**

In systems, where the input is bi-polar, the THS4031 can be used in the inverting configuration with an additional DC bias applied to its + input so as to keep the input to the ADS8481 within its rated operating voltage range. This configuration is also recommended when the ADS8481 is used in signal processing applications where good SNR and THD performance is required. The DC bias can be derived from the REF3220 or the REF3240 reference voltage ICs. The input configuration shown below is capable of delivering better than 92dB SNR and -100db THD at an input frequency of 100 kHz. In case band-pass filters are used to filter the input, care should be taken to ensure that the signal swing at the input of the band-pass filter is small so as to keep the distortion introduced by the filter minimal. In such cases, the gain of the circuit shown below can be increased to keep the input to the ADS8481 large to keep the SNR of the system high. Note that the gain of the system from the + input to the output of the THS4031 in such a configuration is a function of the gain of the AC signal. A resistor divider can be used to scale the output of the REF3220 or REF3240 to reduce the voltage at the DC input to THS4031 to keep the voltage at the input of the converter within its rated operating range.

## PRINCIPLES OF OPERATION (continued)

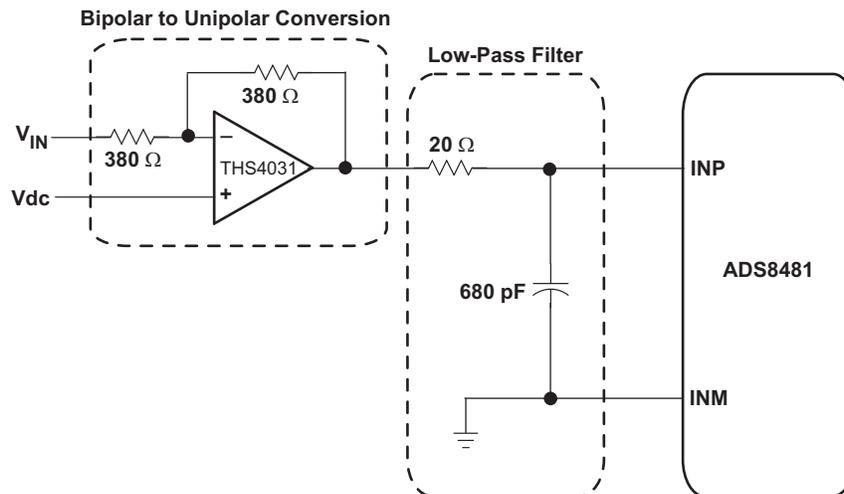


Figure 41. Input Circuit

## DIGITAL INTERFACE

### Timing and Control

See the timing diagrams in the specifications section for detailed information on timing signals and their requirements.

The ADS8481 uses an internal oscillator generated clock which controls the conversion rate and in turn the throughput of the converter. No external clock input is required.

Conversions are initiated by bringing the  $\overline{\text{CONVST}}$  pin low for a minimum of 20 ns (after the 20 ns minimum requirement has been met, the  $\overline{\text{CONVST}}$  pin can be brought high), while  $\overline{\text{CS}}$  is low. The ADS8481 switches from the sample to the hold mode on the falling edge of the  $\overline{\text{CONVST}}$  command. A clean and low jitter falling edge of this signal is important to the performance of the converter. The  $\overline{\text{BUSY}}$  output is brought high immediately following  $\overline{\text{CONVST}}$  going low.  $\overline{\text{BUSY}}$  stays high throughout the conversion process and returns low when the conversion has ended.

Sampling starts with the falling edge of the  $\overline{\text{BUSY}}$  signal when  $\overline{\text{CS}}$  is tied low or starts with the falling edge of  $\overline{\text{CS}}$  when  $\overline{\text{BUSY}}$  is low.

Both  $\overline{\text{RD}}$  and  $\overline{\text{CS}}$  can be high during and before a conversion with one exception ( $\overline{\text{CS}}$  must be low when  $\overline{\text{CONVST}}$  goes low to initiate a conversion). Both the  $\overline{\text{RD}}$  and  $\overline{\text{CS}}$  pins are brought low in order to enable the parallel output bus with the conversion.

### Reading Data

The ADS8481 outputs full parallel data in straight binary format as shown in Table 1. The parallel output is active when  $\overline{\text{CS}}$  and  $\overline{\text{RD}}$  are both low. There is a minimal quiet zone requirement around the falling edge of  $\overline{\text{CONVST}}$ . This is 50 ns prior to the falling edge of  $\overline{\text{CONVST}}$  and 40 ns after the falling edge. No data read should be attempted within this zone. Any other combination of  $\overline{\text{CS}}$  and  $\overline{\text{RD}}$  sets the parallel output to 3-state.  $\overline{\text{BYTE}}$  and  $\overline{\text{BUS18/16}}$  are used for multiword read operations.  $\overline{\text{BYTE}}$  is used whenever lower bits on the bus are output on the higher byte of the bus.  $\overline{\text{BUS18/16}}$  is used whenever the last two bits on the 18-bit bus are output on either bytes of the higher 16-bit bus. Refer to Table 1 for ideal output codes.

**Table 1. Ideal Input Voltages and Output Codes**

DESCRIPTION	ANALOG VALUE	DIGITAL OUTPUT STRAIGHT BINARY	
		BINARY CODE	HEX CODE
Full scale range	$+V_{ref}$		
Least significant bit (LSB)	$(+V_{ref})/262144$		
+Full scale	$(+V_{ref}) - 1 \text{ LSB}$	11 1111 1111 1111 1111	3FFFF
Midscale	$(+V_{ref})/2$	10 0000 0000 0000 0000	20000
Midscale - 1 LSB	$(+V_{ref})/2 - 1 \text{ LSB}$	01 1111 1111 1111 1111	1FFFF
Zero	0 V	00 0000 0000 0000 0000	00000

The output data is a full 18-bit word (D17–D0) on DB17–DB0 pins (MSB–LSB) if both  $\overline{\text{BUS18/16}}$  and  $\overline{\text{BYTE}}$  are low.

The result may also be read on an 16-bit bus by using only pins DB17–DB2. In this case two reads are necessary: the first as before, leaving both  $\overline{\text{BUS18/16}}$  and  $\overline{\text{BYTE}}$  low and reading the 16 most significant bits (D17–D2) on pins DB17–DB2, then bringing  $\overline{\text{BUS18/16}}$  high while holding  $\overline{\text{BYTE}}$  low. When  $\overline{\text{BUS18/16}}$  is high, the lower two bits (D1–D0) appear on pins DB3–DB2.

The result may also be read on an 8-bit bus for convenience. This is done by using only pins DB17–DB10. In this case three reads are necessary: the first as before, leaving both  $\overline{\text{BUS18/16}}$  and  $\overline{\text{BYTE}}$  low and reading the 8 most significant bits on pins DB17–DB10, then bringing  $\overline{\text{BYTE}}$  high while holding  $\overline{\text{BUS18/16}}$  low. When  $\overline{\text{BYTE}}$  is high, the medium bits (D9–D2) appear on pins DB17–DB10. The last read is done by bringing  $\overline{\text{BUS18/16}}$  high while holding  $\overline{\text{BYTE}}$  high. When  $\overline{\text{BUS18/16}}$  is high, the lower two bits (D1–D0) appear on pins DB11–DB10. The last read cycle is not necessary if only the first 16 most significant bits are of interest.

All of these multiword read operations can be performed with multiple active  $\overline{\text{RD}}$  (toggling) or with  $\overline{\text{RD}}$  held low for simplicity. This is referred to as the AUTO READ operation.

**Table 2. Conversion Data Read Out**

BYTE	BUS18/16	DATA READ OUT				
		PINS DB17–DB12	PINS DB11–DB10	PINS DB9–DB4	PINS DB3–DB2	PINS DB1–DB0
High	High	All One's	D1–D0	All One's	All One's	All One's
Low	High	All One's	All One's	All One's	D1–D0	All One's
High	Low	D9–D4	D3–D2	All One's	All One's	All One's
Low	Low	D17–D12	D11–D10	D9–D4	D3–D2	D1–D0

## RESET

On power-up, internal POWER-ON RESET circuitry generates the reset required for the device. The first three conversions after power-up are used to load factory trimming data for a specific device to assure high accuracy of the converter. The results of the first three conversions are invalid and should be discarded.

The device can also be reset through the use of the combination for  $\overline{\text{CS}}$  and  $\overline{\text{CONVST}}$ . Since the  $\overline{\text{BUSY}}$  signal is held at high during the conversion, either one of these conditions triggers an internal self-clear reset to the converter.

- Issue a  $\overline{\text{CONVST}}$  when  $\overline{\text{CS}}$  is low and the internal convert state is high. The falling edge of  $\overline{\text{CONVST}}$  starts a reset.
- Issue a  $\overline{\text{CS}}$  (select the device) while the internal convert state is high. The falling edge of  $\overline{\text{CS}}$  causes a reset.

Once the device is reset, all output latches are cleared (set to zeroes) and the  $\overline{\text{BUSY}}$  signal is brought low. A new sampling period is started at the falling edge of the  $\overline{\text{BUSY}}$  signal immediately after the instant of the internal reset.

**LAYOUT**

For optimum performance, care must be taken with the physical layout of the ADS8481 circuitry.

As the ADS8481 offers single-supply operation, it is often used in close proximity with digital logic, microcontrollers, microprocessors, and digital signal processors. The more digital logic present in the design and the higher the switching speed, the more difficult it is to achieve good performance from the converter.

The basic SAR architecture is sensitive to glitches or sudden changes on the power supply, reference, ground connections and digital inputs that occur just prior to latching the output of the analog comparator. Thus, driving any single conversion for an n-bit SAR converter, there are at least n windows in which large external transient voltages can affect the conversion result. Such glitches might originate from switching power supplies, nearby digital logic, or high power devices.

The degree of error in the digital output depends on the reference voltage, layout, and the exact timing of the external event.

On average, the ADS8481 draws very little current from an external reference as the reference voltage is internally buffered. If the reference voltage is external and originates from an op amp, make sure that it can drive the bypass capacitor or capacitors without oscillation. A 0.1-μF capacitor is recommended from pin 13 (REFIN) directly to pin 12 (REFM). REFM and AGND must be shorted on the same ground plane under the device.

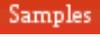
The AGND and BDGND pins should be connected to a clean ground point. In all cases, this should be the analog ground. Avoid connections which are too close to the grounding point of a microcontroller or digital signal processor. If required, run a ground trace directly from the converter to the power supply entry point. The ideal layout consists of an analog ground plane dedicated to the converter and associated analog circuitry.

As with the AGND connections, +VA should be connected to a 5-V power supply plane or trace that is separate from the connection for digital logic until they are connected at the power entry point. Power to the ADS8481 should be clean and well bypassed. A 0.1-μF ceramic bypass capacitor should be placed as close to the device as possible. See [Table 3](#) for the placement of the capacitor. In addition, a 1-μF to 10-μF capacitor is recommended. In some situations, additional bypassing may be required, such as a 100-μF electrolytic capacitor or even a Pi filter made up of inductors and capacitors—all designed to essentially low-pass filter the 5-V supply, removing the high frequency noise.

**Table 3. Power Supply Decoupling Capacitor Placement**

POWER SUPPLY PLANE	CONVERTER ANALOG SIDE	CONVERTER DIGITAL SIDE
SUPPLY PINS		
Pin pairs that require shortest path to decoupling capacitors	(7,8), (9,10), (16,17), (20,21), (22,23), (25,26)	36, 37
Pins that require no decoupling	24, 26	1

**PACKAGING INFORMATION**

Orderable Device	Status (1)	Package Type	Package Drawing	Pins	Package Qty	Eco Plan (2)	Lead finish/ Ball material (6)	MSL Peak Temp (3)	Op Temp (°C)	Device Marking (4/5)	Samples
ADS8481IBRGZT	ACTIVE	VQFN	RGZ	48	250	RoHS & Green	Call TI	Level-2-260C-1 YEAR	-40 to 85	ADS 8481I B	
ADS8481IBRGZTG4	ACTIVE	VQFN	RGZ	48	250	RoHS & Green	Call TI	Level-2-260C-1 YEAR	-40 to 85	ADS 8481I B	

(1) The marketing status values are defined as follows:

**ACTIVE:** Product device recommended for new designs.

**LIFEBUY:** TI has announced that the device will be discontinued, and a lifetime-buy period is in effect.

**NRND:** Not recommended for new designs. Device is in production to support existing customers, but TI does not recommend using this part in a new design.

**PREVIEW:** Device has been announced but is not in production. Samples may or may not be available.

**OBSOLETE:** TI has discontinued the production of the device.

(2) **RoHS:** TI defines "RoHS" to mean semiconductor products that are compliant with the current EU RoHS requirements for all 10 RoHS substances, including the requirement that RoHS substance do not exceed 0.1% by weight in homogeneous materials. Where designed to be soldered at high temperatures, "RoHS" products are suitable for use in specified lead-free processes. TI may reference these types of products as "Pb-Free".

**RoHS Exempt:** TI defines "RoHS Exempt" to mean products that contain lead but are compliant with EU RoHS pursuant to a specific EU RoHS exemption.

**Green:** TI defines "Green" to mean the content of Chlorine (Cl) and Bromine (Br) based flame retardants meet JS709B low halogen requirements of <=1000ppm threshold. Antimony trioxide based flame retardants must also meet the <=1000ppm threshold requirement.

(3) MSL, Peak Temp. - The Moisture Sensitivity Level rating according to the JEDEC industry standard classifications, and peak solder temperature.

(4) There may be additional marking, which relates to the logo, the lot trace code information, or the environmental category on the device.

(5) Multiple Device Markings will be inside parentheses. Only one Device Marking contained in parentheses and separated by a "-" will appear on a device. If a line is indented then it is a continuation of the previous line and the two combined represent the entire Device Marking for that device.

(6) Lead finish/Ball material - Orderable Devices may have multiple material finish options. Finish options are separated by a vertical ruled line. Lead finish/Ball material values may wrap to two lines if the finish value exceeds the maximum column width.

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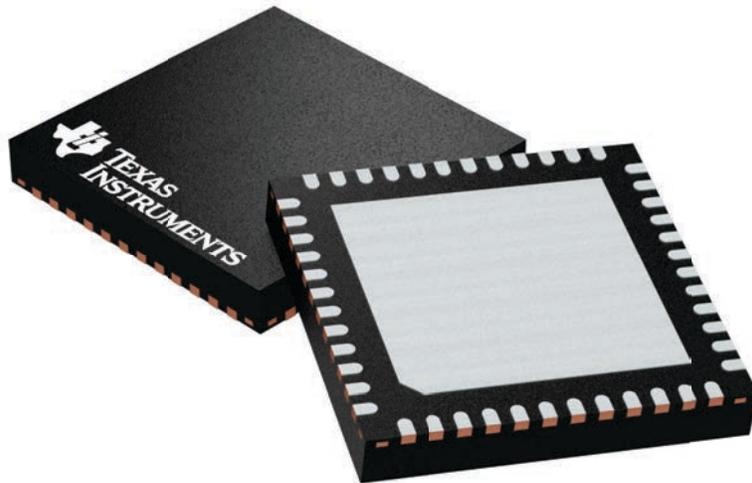
## GENERIC PACKAGE VIEW

**RGZ 48**

**VQFN - 1 mm max height**

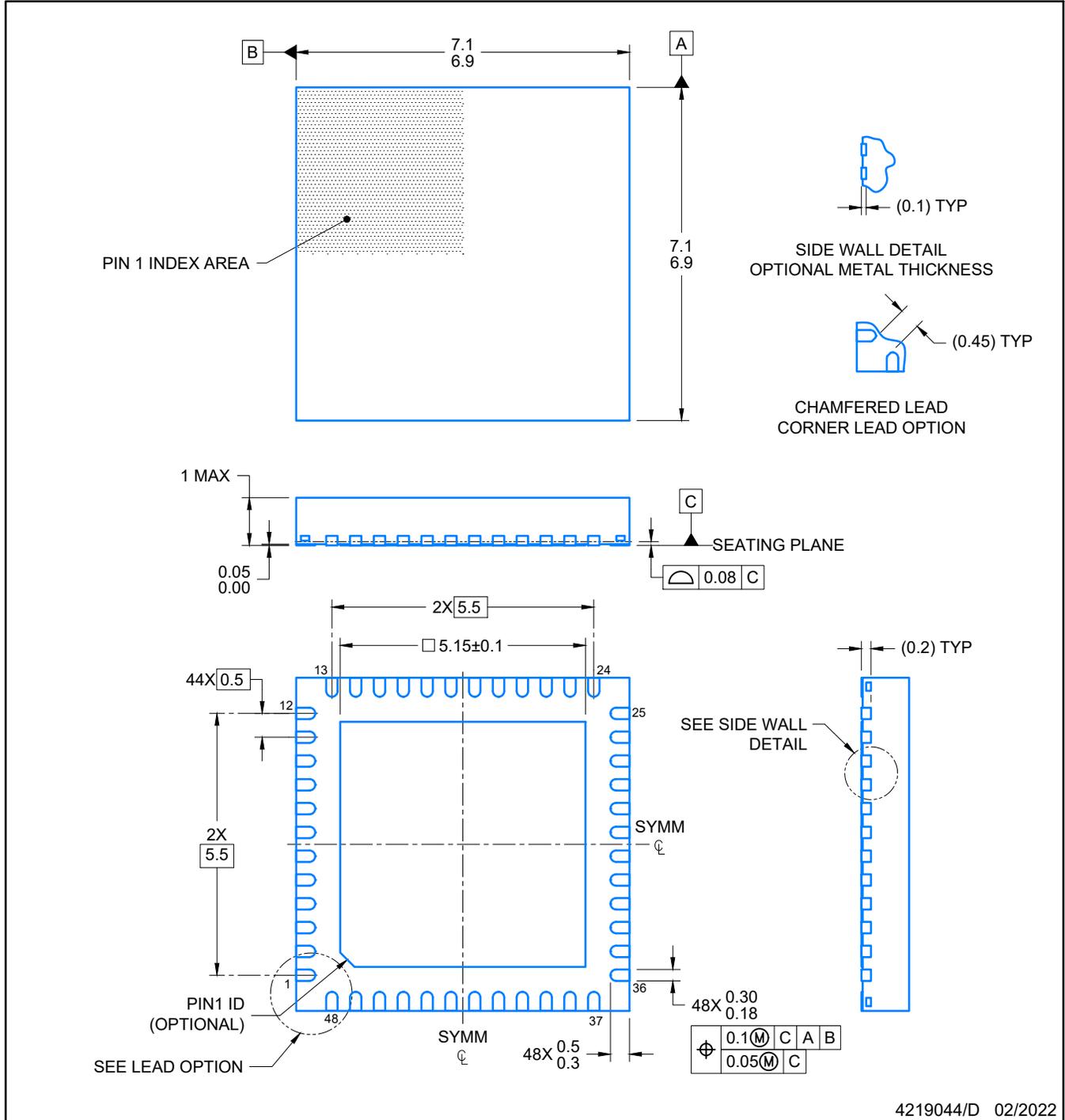
7 x 7, 0.5 mm pitch

PLASTIC QUADFLAT PACK- NO LEAD



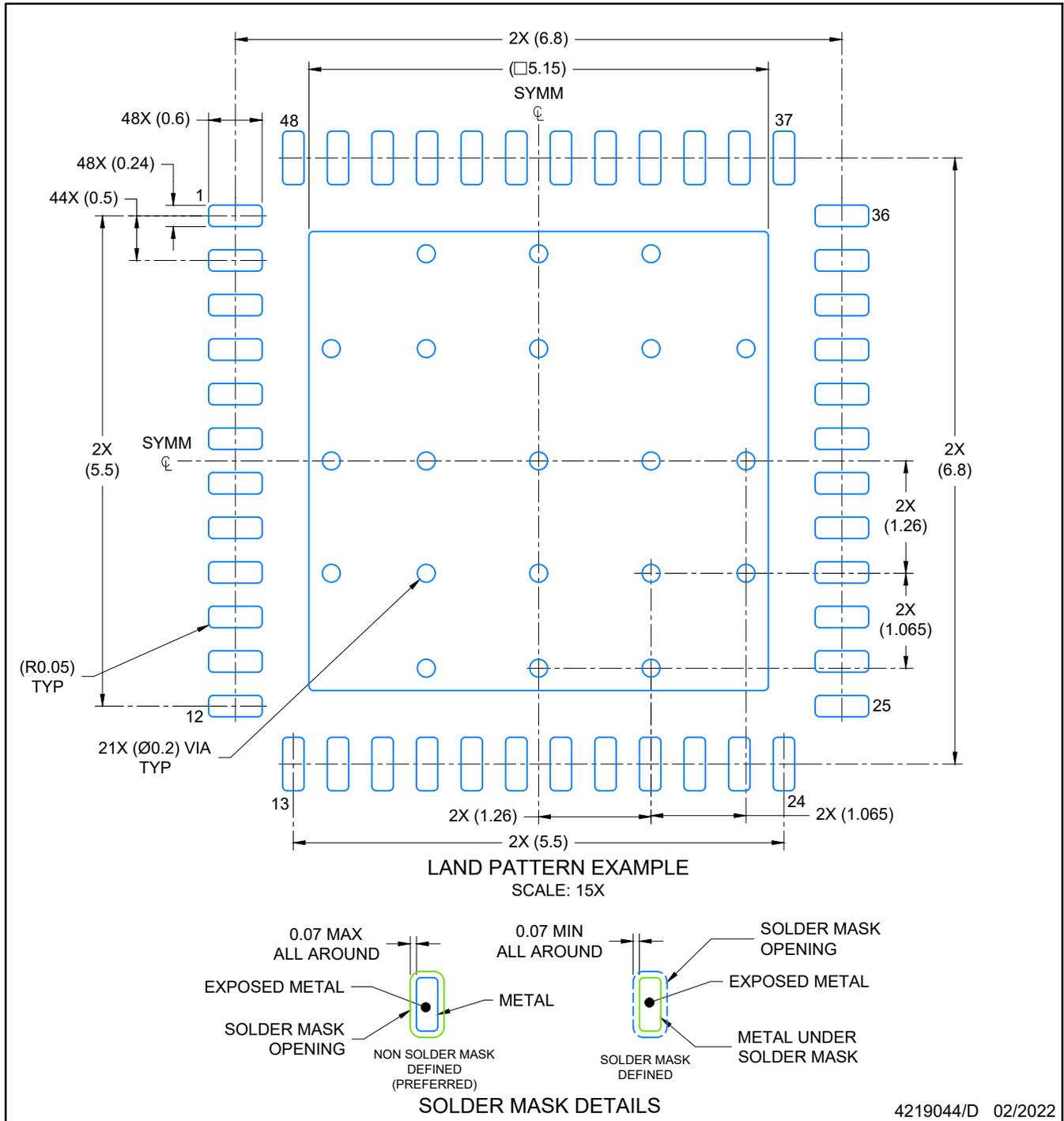
Images above are just a representation of the package family, actual package may vary.  
Refer to the product data sheet for package details.

4224671/A



NOTES:

1. All linear dimensions are in millimeters. Any dimensions in parenthesis are for reference only. Dimensioning and tolerancing per ASME Y14.5M.
2. This drawing is subject to change without notice.
3. The package thermal pad must be soldered to the printed circuit board for optimal thermal and mechanical performance.



NOTES: (continued)

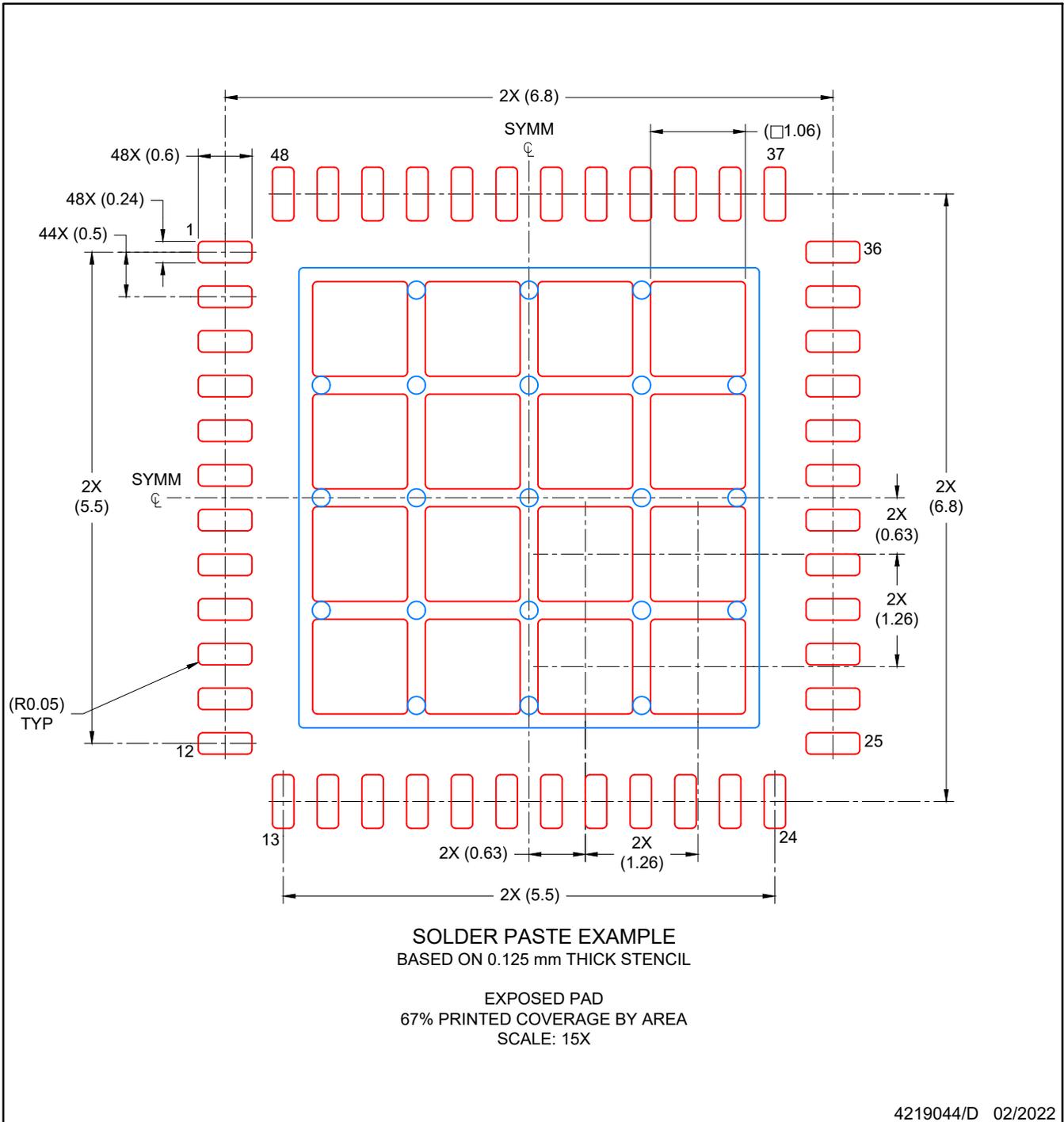
4. This package is designed to be soldered to a thermal pad on the board. For more information, see Texas Instruments literature number SLUA271 ([www.ti.com/lit/slua271](http://www.ti.com/lit/slua271)).
5. Vias are optional depending on application, refer to device data sheet. If any vias are implemented, refer to their locations shown on this view. It is recommended that vias under paste be filled, plugged or tented.

# EXAMPLE STENCIL DESIGN

RGZ0048A

VQFN - 1 mm max height

PLASTIC QUADFLAT PACK- NO LEAD



NOTES: (continued)

6. Laser cutting apertures with trapezoidal walls and rounded corners may offer better paste release. IPC-7525 may have alternate design recommendations.

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